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All-Band 2G+3G Radial Disc-Cone Antennas: Design, Construction and Measurements

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EECE Dept, Democritus University of Thrace, Hellas [2 and 3]

Abstract

We define as "All-Band 2G+3G" any band that includes all frequencies allocated to both 2G and 3G services. We define as "Radial Disc-Cone Antenna RDCA" any discone antenna with a structure of radial wires. The RDCA was theoretically analyzed and software simulated with the purpose of computationally design a broadband model of it. As an application, a broadband RDCA for operation from 800 to 3,000 MHz, which include all 2G and 3G frequencies, was designed and an experimental model was constructed and tested. In order to evaluate the agreement between theory and practice, mathematically expressed measurement error bounds were computed.

Introduction

In 1945, Kandoian invented the well-known discone antenna, that is a dipole made of a disc above a cone [1]. In 1953, Nail gave experimentally two naive relations for the discone dimensions [2].

In 1987, Rappaport designed discones using an N-type connector feed [3]. In 1993, Cooke studied a discone with a structure of radial wires [4]. In 2005, Kim et al. presented a double radial discone antenna for Ultra Wide-Band applications [5].

In this short paper we present an All-Band 2G+3G RDCA fed by an N—type/Female/50—Ohm connector.

Research

The RDCA was theoretically analyzed as a group of identical filamentary V-dipoles with unequal arms connected in parallel. The dipoles recline on equiangular vertical phi-planes around z-axis to form a disconical array. Fig.1A shows two such coplanar dipoles conformed with the apex angle a. Each V-dipole has a total length L equal to the sum of arm lengths r and s plus the gap g between its terminals.

The simulation was based on a suite of developed visual tools which are supported by a fully analyzed, corrected and redeveloped edition of the original thin-wire computer program by J.H. Richmond [6].

Two arithmetic criteria were adopted for the broadband characterization of a model:

(1) 50-Ohm VSWR lower than 2
(2) Normalized radiation intensity U/Umax lower than 3 dB on the horizontal plane.

A visual application program was specifically developed to design a broadband radial discone with bare wires of diameter d embedded in free space when the wire conductivity, the type of feeding connector and the frequency band are given.

The program uses the model of a radial discone fed by an N-type connector shown in Fig.2. Starting with an appropriate combination of the relations given by [2]-[4] the program computes by iteration in terms of wavelength λ, the geometric characteristics r, s, g, a, of the broadband model, just when the criteria are satisfied.

Fig.1B shows a Ground Plane Antenna GPA that was designed for reference and consists of equal number of cone radials s and a vertical monopole with height r.

As a practical application of the broadband design, the 2G+3G band from 800 to 2,500 MHz was selected to begin with and an experimental radial discone of copper wire fed by N-type connector was built, as shown in Fig.3.

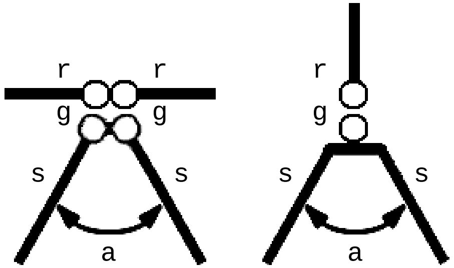

Fig.1: A — RDCA, B — GPA

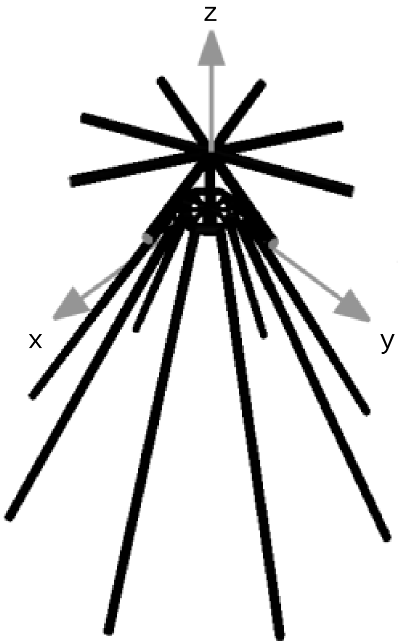

Fig.2: RDCA — Designed Model

In order to demonstrate the particular behavior of the experimental model, the 2G+3G band was divided as follows:

2G+3G Sub-Bands
800 MHz — 2,500 MHz

Sub-Band	MHz
I	806 — 960
II	1,429 — 1,513
III	1,710 — 1,900
IV	1,910 — 2,025
V	2,110 — 2,170
VI	2,400 — 2,499

Our measurement system consists of an EM anechoic chamber, a network analyzer, a number of support instruments, a set of standard loads of factory accuracy and a constructed antenna rotation mechanism with a built hardware control unit of its step motor. The combined characteristics of system parts specify a measurement band from 600 to 1300 MHz, which overlaps with the 2G/3G band. Developed control software synchronizes the system and collects data using the IEEE-488 protocol.

A developed general mathematical method expresses the measurement error bounds. Another set of developed software applications processes the collected data and computes the error bounds.

Results

The consideration of radial discone as an array of at least eight 8 V-dipoles produces a theta-polarized vector radiation pattern with magnitude a surface almost by revolution around z-axis. So the radial discone has indeed on the horizontal plane xOy the basic properties of a vertically polarized almost omni-directional antenna, that is a fact that encouraged the design of a broadband model by using simulation.

The application of the broadband criteria to 2G/3G band resulted to the design of a RDCA with the following geometrical characteristics:

All-Band 2G+3G RDCA
800 MHz — 3,000 MHz

Geometry		Units
d	1.5	[mm]
r	44	[mm]
g	6	[mm]
s	125	[mm]
a	60	[°]

The RDCA operates from 800 to 3,000 MHz, which exceeds that of 2G+3G band. The accordingly constructed experimental radial discone of Fig.3 should be implied with a constructional tolerance of ±0.5 mm and ±0.5°.

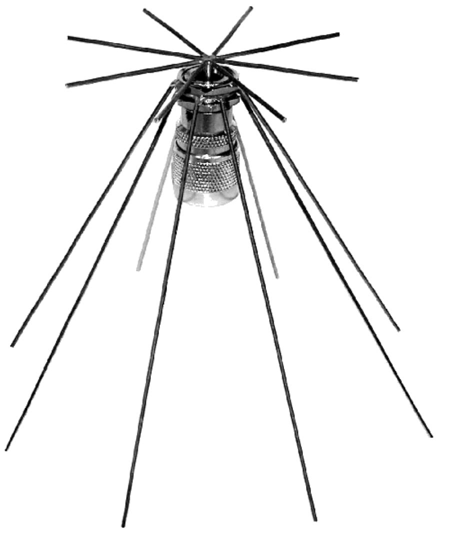

Fig.3: RDCA experimental model

The broadband model has a directivity from about −0.5 to 2.9 dBd with slope angle between −65° and +58°, but the directivity gain on horizontal plane stays very close to the desirable value of 0 dBi, since it changes from −1 to +1.7 dBi only. Fig.4 shows that the predicted horizontal normalized radiation intensity remains below 3 dB indeed, while it stays above 0 dB relative to the reference antenna in all 2G+3G sub-bands indicated by the vertical gray strips, when both are fed by the same 50-Ohm source.

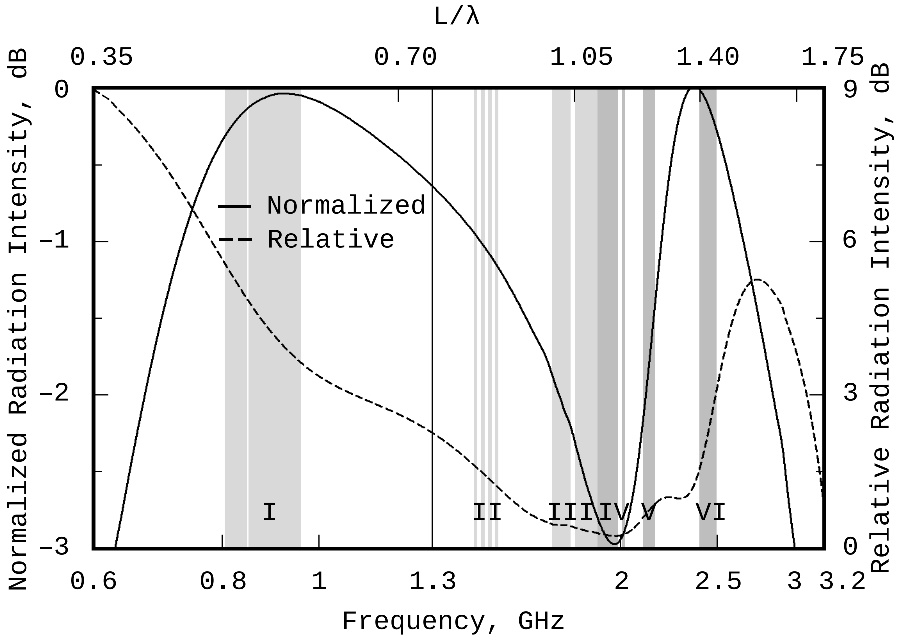

Fig.4: Predicted radiation intensity on horizontal plane.

Fig.5A shows the predicted normalized radiation patterns in dB at the center of each sub-band, which confirms the horizontal omni-directional radiation properties of the broadband model.

At the center frequency of 950 MHz of the measurement band, the predicted and measured radiation intensity on the three main cuts of the radiation pattern are in good agreement, as shown in Fig. 5B.

This is made clearer by the measurement error bounds on a vertical plane as shown in Fig.6.

Fig.7 shows that the 50-Ohm VSWR predicted results for the broadband discone are below 2 indeed and almost covered by the error bounds in the measurement band.

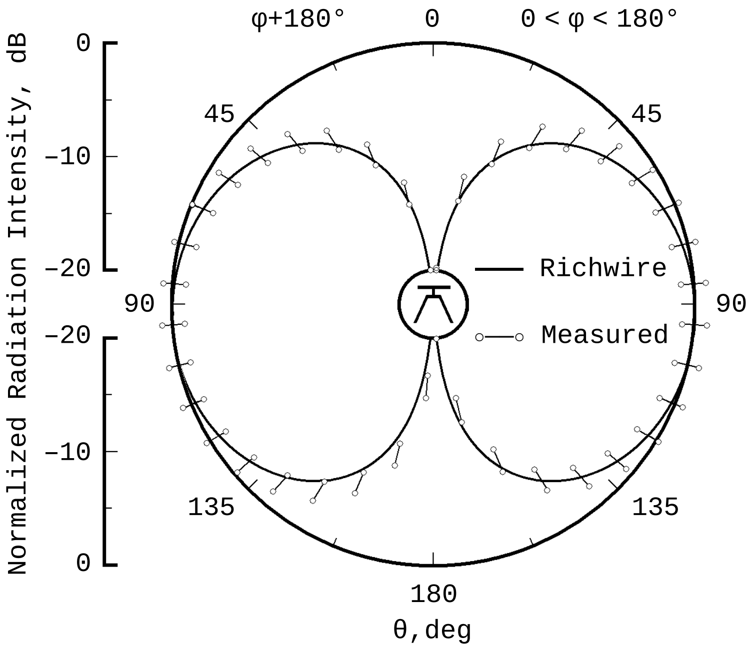

Fig.6: Measurement error bounds on a vertical plane

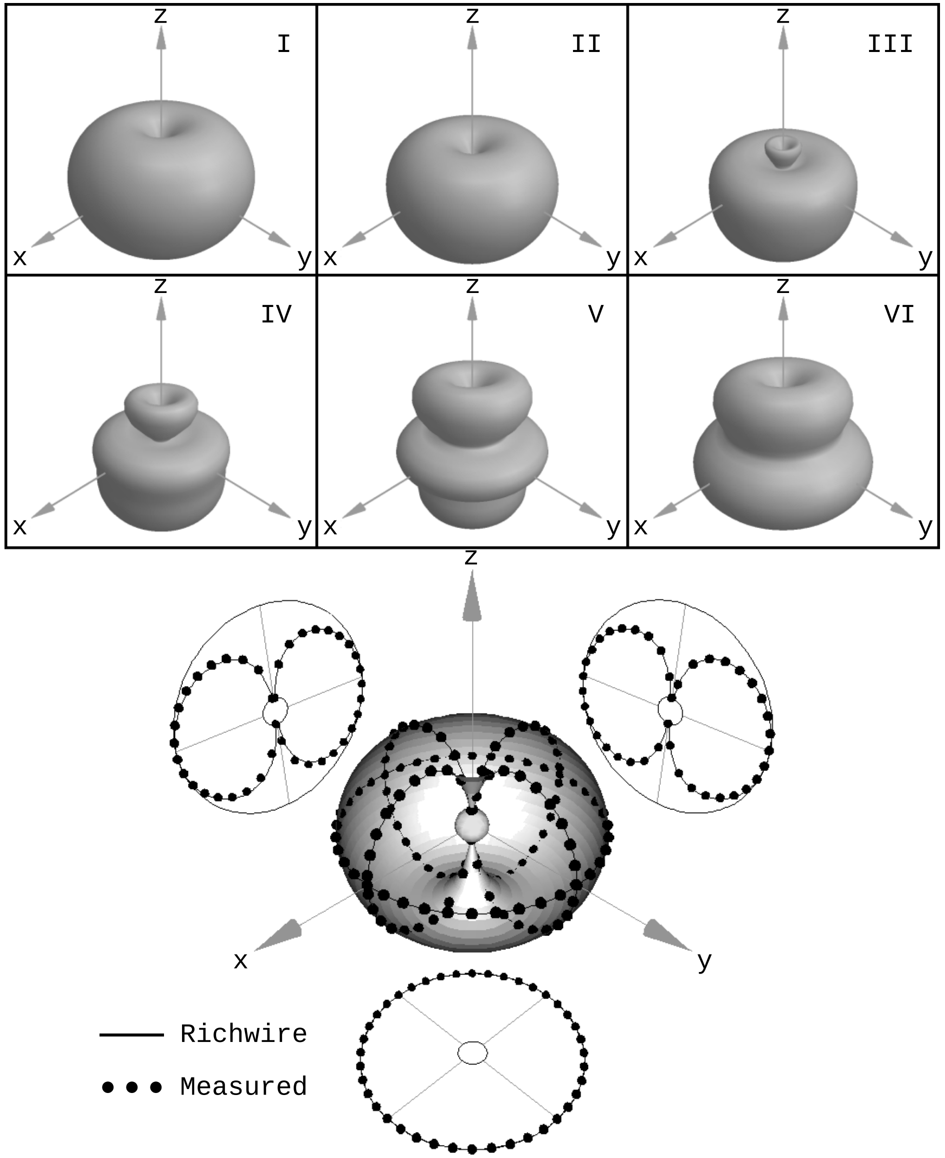

Fig.5: A (Up) Predicted normalized radiation intensity patterns at the center of each 2G+3G sub-band – B (Down) Normalized radiation intensity pattern at the center of measurements band

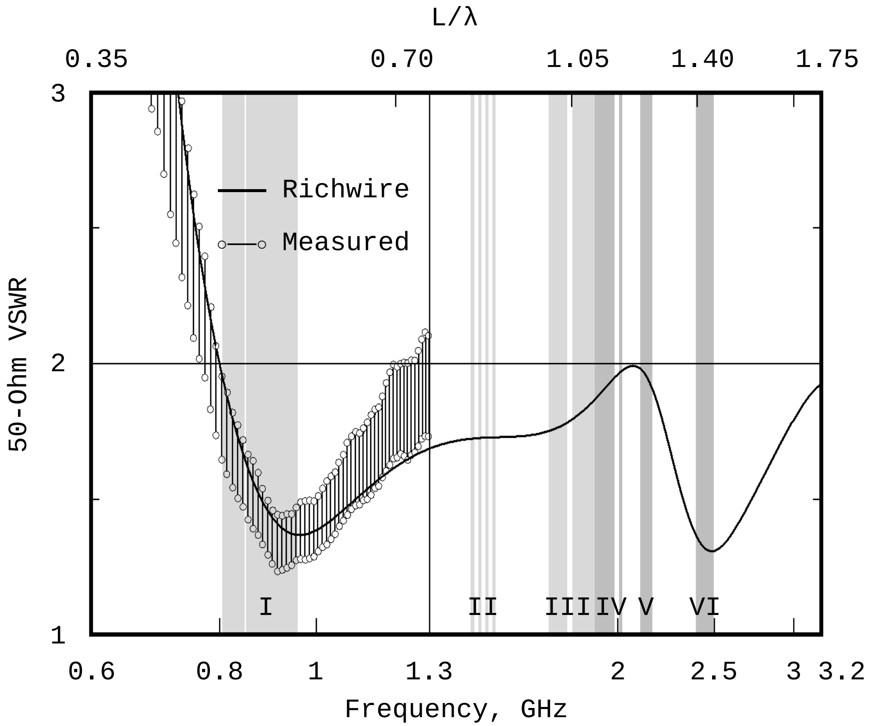

Fig.7: Standing wave ratio against frequency or ratio of total length to wavelength

Conclusion

Prediction and experimentation in the measurement band 600 MHz to 1,300 MHz proposes a successfully designed, constructed, and measured Radial Disk Cone Antenna RDCA capable to serve All-Band 2G+3G applications from 800 MHz to 3,000 MHz.

Credits

The authors acknowledge Adamantios Diamantidis, SV7FSF, a former member of Computer Center – Network Administration Center at Democritus University of Thrace, now Systems Engineer, Systems Administrator (honorary), Berlin, Germany, who motivated the study of Discone Antennas on behalf of FSF Free Software Foundation followers on the purpose to be openly supported in their Wi-Fi activities.

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Broadband radial discone antenna:
Design, application and measurements
N. I. Yannopoulou, P. E. Zimourtopoulos, E. T. Sarris
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Measurement Uncertainty in Network Analyzers: Differential Error Analysis of Error Models
Part 1: Full One-Port Calibration

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Abstract

An analytical method was developed to estimate errors in quantities depended on full one-port vector network analyzer (VNA) measurements using differentials and a complex differential error region (DER) was defined. To evaluate the method, differences instead of differentials were placed over a DER which was then analyzed and compared with another commonly used estimated error. Two real differential error intervals (DEIs) were defined by the greatest lower and least upper bounds of DER projections. To demonstrate the method, a typical device under test (DUT) was built and tested against frequency. Practically, a DER and its DEIs are solely based on manufacturer's data for standard loads and their uncertainties, measured values and their inaccuracies.

Introduction

In full one-port measurements with a VNA of real characteristic impedance Z_0, a DUT with impedance Z has a reflection coefficient ρ defined by

$$\rho = (Z - Z_0)/(Z + Z_0)$$

and related to its measured value m by the bilinear transformation

$$\rho = (m - D)/[M(m - D) + R]$$

in terms of errors D, M and R [1]. This transformation can be uniquely determined from given distinct ρ_n, n = 1, 2, 3 and respectively known m_k, k = n [2].

Research

We considered ρ_n, m_k as the elements of given ordered triples (A, B, C), (a, b, c), solved the resulting system and appropriately expressed its solution by

$$F = \sum cC(B - A)$$

$$D = \sum abC(A - B)/F$$

$$M = \sum c(B - A)/F$$

$$R = [\prod (A - B)(a - b)]/F^2$$

where ∑ and ∏ produce two more terms from the one shown, by rotation of the ordered triple elements. These errors were then considered

as depended on the independent variables ρ_n, m_k. Therefore, their differentials were expressed in the same manner by

$$\begin{aligned} dD = [&\prod (a - b) \sum (B - C)BC\, dA \\ &+ \sum (b - c)^2(B - A)(C - A) \\ &BC\, da]/F^2 \end{aligned}$$

$$\begin{aligned} dM = [&\sum (a - b)(c - a)(B - C)^2 dA \\ &- \prod (A - B) \sum (b - c)da]/F^2 \end{aligned}$$

$$\begin{aligned} dR = \{&\sum [F + 2(a - b)B(A - C)] \\ &[(B - C)^2 dA \prod (a - b) \\ &- (b - c)^2 da \prod (A - B)]\}/F^3 \end{aligned}$$

After that, the differential of ρ was expressed by

$$\begin{aligned} d\rho = [&-RdD - (m - D)^2 dM - (m - D)dR \\ &+ Rdm]/[M(m - D) + R]^2 \end{aligned}$$

and was considered depended, through dD, dM and dR, on L = 7 independent variables and their independent differentials: ρ_n, n = 1, 2, 3 and m_k, k = n or k = 0 with $m_0 = m$.

The developed expressions were mechanically verified using a developed software program for symbolic computations.

Manufacturer's data for standard loads used in full-one port VNA measurements are substituted in ρ_n, and for their uncertainties in $d\rho_n$. Since Z_0 is real, the domain of each ρ_n is the closed unit circle [3]. For $|\rho_n| = 0$ or 1, care must be exercised to restrict its differential value onto its domain. The VNA measurements have specified bounded ranges for their modulus and argument, so that the domain of each m_k is a bounded circular annular with its center at the origin Ο of the complex plane. Measurement data are substituted in m_k and manufacturer's data for measurement inaccuracy in dm_k. Uncertainty and inaccuracy data outline domains for $d\rho_n$ and dm_k. If $z = |r|e^{j\varphi}$, stands for any of the independent variables and dz for its differential then the contribution of dz to dρ is a summation term of the form Wdz, with $W = |U|e^{jV}$, so that

$$\begin{aligned} Wdz = &|U|e^{j(V + \varphi)} d|r| \\ &+ |U|e^{j(V + \varphi + \pi/2)} |r| d\varphi \end{aligned}$$

where W is in fact a known value of the respective partial derivative and d|r|, dφ are the independent real differentials of the complex dz in polar form. Each expression Wdz outlines a contour for a partial DER around Ο. If $z \neq 0$, the partial DER is a parallelogram with perpendicular sides d|r| and |r|dφ, stretched or contracted by |U| and rotated by (V + φ) around Ο. If $z = \rho_n = 0$, the partial DER is a circle with radius |U|d|r|. Accordingly, a DER is the sum of either L parallelograms or (L – 1) parallelograms and 1 circle. DER is then a convex set with contour either a polygonal line with 4L vertices at most, or a piecewise curve composed of 4(L – 1) line segments and 4(L – 1) circular arcs at most. The greatest lower and least upper differential error bounds are the end-points of DEIs for the real and imaginary parts of dρ and result from the projections of DER for ρ on the coordinate axes. These conclusions can be generalized for any other quantity directly or indirectly depended on all, some or just one of the above independent variables and their differentials. Thus, the quantity has an L-term DER, where $7 \ge L \ge 1$. For example, the impedance Z of a DUT has the 7-term DER:

$$dZ = 2Z_0 d\rho/(1-\rho)^2$$

Results

All of the following data are specified by manufacturers of the parts for our measurement system. This system operates from 1 to 1300 MHz with 100 Hz PLL stability and consists of a type-N $Z_0 = 50\ \Omega$ network analyzer, a number of support instruments and a set of standard loads. The standards are: a short circuit A, a matching load B with reflection coefficient 0.029 and an open circuit C with reflection coefficient 0.99 and phase accuracy ±2°. In the absence of manufacturer's data for A we considered its uncertainty equal to that of C. So, the following values were substituted in the developed expressions:

$A = -1,\ 0 \le d|A| \le 0.01,\ -180° \le d\varphi_A \le -178°$ or $178° \le d\varphi_A \le 180°$,

$B = 0,\ |dB| = 0.029$,

$C = 1,\ -0.01 \le d|C| \le 0,\ -2° \le d\varphi_C \le +2°$

The annular domain for m_k of VNA is specified from 0 to –70 db in modulus and ±180 degrees in argument. Measurements m_k result with a decimal floating point precision of 4 digits, for both modulus and argument. We consider the modulus and argument of dm_k equal to ±1/2 of the unit in the last place of the corresponding mantissa in modulus and argument of m_k Consequently, our system produces a DER, either for ρ or Z, as a sum of $(L-1) = 6$ parallelograms and 1 circle, with a contour of $(4L + 4L) = 48$ vertices at most.

A suite of developed software applications: (i) controls the system and collects the data in terms of frequency using the IEEE-488 protocol, (ii) processes the collected data and computes the vertices of DER and the end-points of its DEIs (iii) sketches pictures of DER for ρ and Z in terms of the frequency steps and make a film using them as frames.

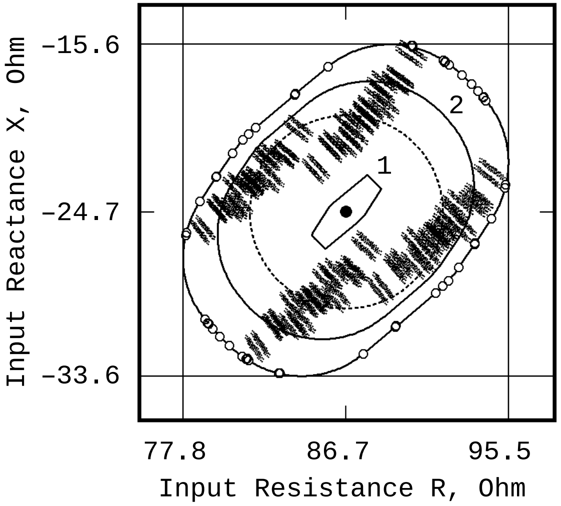

Fig.1: A typical DER for the impedance Z

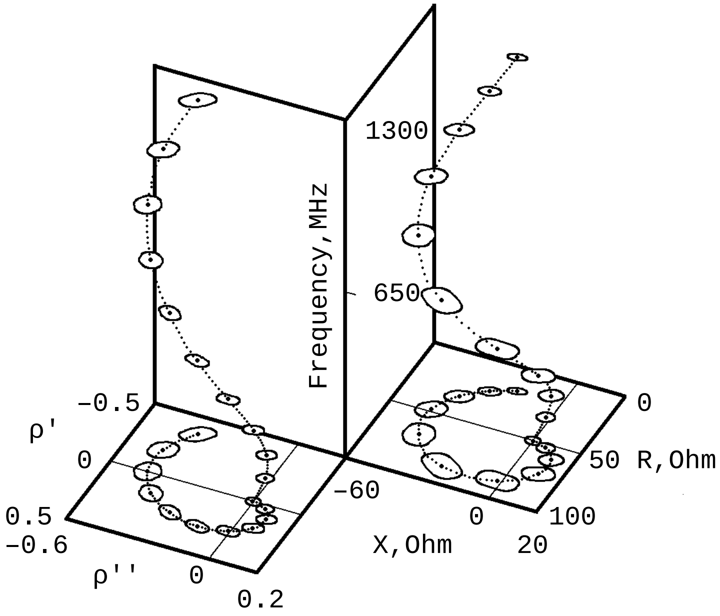

Fig.2: DER for the reflection coefficient ρ and for its associated impedance Z against frequency

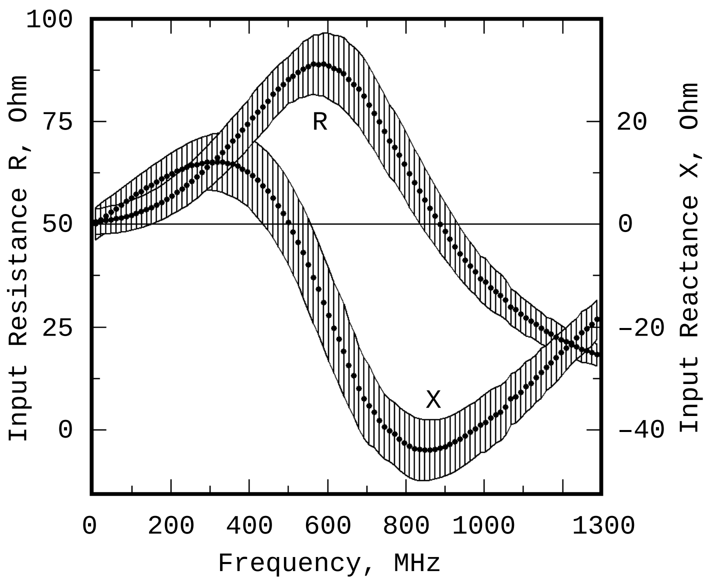

Fig.3: Greatest lower and least upper differential error bounds for resistance R and reactance X against frequency

A typical resistor with a nominal DC impedance of 50 Ω ±20% tolerance was soldered on a type-N base connector and enclosed in an aluminium box to serve as a simple DUT for testing its Z from 2 to 1289 MHz in 13 MHz steps. The center frequency f_C = 639 MHz was chosen to reveal the details of the proposed method in Fig.1, where the contour of a typical DER for Z is outlined with small circles as its vertices. This contour surrounds that of the 4-terms DER due to inaccuracy of measurements (1) and that of 3-terms DER for the uncertainty of loads (2). A properly circumscribed rectangle of DER shows graphically how the DEIs for R and X result. The commonly used error from the matching load only is shown as a dotted circle. This is in fact a 1-term DER which is surrounded from the contour of the DER by a factor of about 125% to 185% in all directions. Finally, in the same figure, 2^{7x2} differences ΔZ resulting from the same $d\rho_n$ and dm_k, dense enough to appear as stripes, were placed over DER to compare them with differential dZ values. Notably, almost all of ΔZ values are belong to DER while the computation time for these ΔZ exceeds that for DER by more than one order of magnitude. To demonstrate the method, a set of selected DER frames for ρ and Z are shown in Fig.2, as beads on space curved filaments against frequency.

Finally, the computed DEIs for R and X are shown in Fig.3 against frequency.

Conclusion

The proposed method may be efficiently used in the same way, to successfully estimate errors in any quantity depended on full one-port vector network analyzer measurements.

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Differential Error Region of a Quantity Dependent on
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Measurement Uncertainty in Network Analyzers: Differential Error Analysis of Error Models Part 2: Full Two-Port Calibration

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Abstract

Since S–parameter measurements without uncertainty cannot claim any credibility, the uncertainties in full two–port Vector Network Analyzer (VNA) measurements were estimated using total complex differentials (Total Differential Errors). To express precisely a comparison relation between complex differential errors, their differential error regions (DERs) were used. To demonstrate the method in the most accurate case of a direct zero–length thru, practical results are presented for commonly used Z–parameters of a simple, two–port, DC resistive T–network, which was built and tested against frequency with a VNA measurement system extended by two lengthy transmission lines.

Introduction

It is well known that in full two–port VNA measurements the S–parameters for a two–port Device Under Test (DUT) are given in terms of their 4 measurements m_{ij}, $i = 1, 2$, $j = 1, 2$ by

$$S_{11} = \{[(m_{11} - D)/R][1 + (m_{22} - D')M'/R'] - L(m_{21} - X)(m_{12} - X')/(TT')\}/H \qquad (1)$$

$$S_{21} = \{[1 + (m_{22} - D')(M' - L)/R'](m_{21} - X)/T\}/H \qquad (2)$$

$$H = [1 + (m_{11} - D)M/R][1 + (m_{22} - D')M'/R'] - LL'(m_{21} - X)(m_{12} - X')/(TT') \qquad (3)$$

S_{22}, S_{12} have expressions that result from (1)–(2) by substituting i, j with j, i and D, M, R, L, T, X with D', M', R', T', L', X' and vice–versa [1]. These 12 quantities have been defined as system errors [2]. Stumper gave non–generalized expressions for the partial deviations of S–parameters due to calibration standard uncertainties, in 2003 [3]. Furthermore, the developed total differential errors for full one–port VNA measurements [4] are also not generalized in the two–port case. To the best of the authors' knowledge, there are no analytical expressions for total differential errors in full two–port VNA measurements.

Research

Since S–parameters are functions of 16 complex variables, their total differential errors were initially expressed as

$$\begin{aligned}
dS_{11} = \{&T T'(1 - MS_{11})[R' + M'(m_{22} - D')](dm_{11} - dD)\\
&- RR'L(1 - L'S_{11})[(m_{21} - X)(dm_{12} - dX') + (m_{12} - X')(dm_{21} - dX)]\\
&+ M'T T'[(m_{11} - D)(1 - MS_{11}) - RS_{11}](dm_{22} - dD')\\
&- T T'S_{11}(m_{11} - D)[R' + M'(m_{22} - D')]dM\\
&+ T T'(m_{22} - D')[(m_{11} - D)(1 - MS_{11}) - RS_{11}]dM'\\
&- (R'L(1 - L'S_{11})(m_{12} - X')(m_{21} - X) +\\
&+ T T'S_{11}[R' + M'(m_{22} - D')])dR\\
&- (RL(1 - L'S_{11})(m_{12} - X')(m_{21} - X)\\
&- T T'[(m_{11} - D)(1 - MS_{11}) - RS_{11}])dR'\\
&- RR'(m_{12} - X')(m_{21} - X)[(1 - L'S_{11})dL - LS_{11}dL']\\
&+ [(m_{11} - D)(1 - MS_{11}) - RS_{11}][R' + M'(m_{22} - D')]\\
&(T'dT+TdT')\}/P \qquad (4)
\end{aligned}$$

$$\begin{aligned}
dS_{21} = \{&- MT T'S_{21}[R' + M'(m_{22} - D')](dm_{11} - dD)\\
&+ RR'LL'S_{21}(m_{21} - X)(dm_{12} - dX')\\
&+ R\{T'[R' + (m_{22} - D')(M' - L)] + R'LL'S_{21}(m_{12} - X')\}(dm_{21} - dX)\\
&+ T'(R(m_{21} - X)(M' - L) - M'TS_{21}[R + M(m_{11} - D)])(dm_{22} - dD')\\
&- T T'S_{21}(m_{11} - D)[R' + M'(m_{22} - D')]dM\\
&+ T'(m_{22} - D')(R(m_{21} - X) - TS_{21}[R + M(m_{11} - D)])dM'\\
+ \{&(m_{21} - X)(T'(m_{22} - D')(M' - L) + R'[T' + LL'S_{21}(m_{12} - X')])\\
&- T T'S_{21}[R' + M'(m_{22} - D')]\}dR\\
&+ (R(m_{21} - X)[T' + LL'S_{21}(m_{12} - X')]\\
&- T T'S_{21}[R + M(m_{11} - D)])dR'\\
&+ R(m_{21} - X)[R'L'S_{21}(m_{12} - X') - T'(m_{22} - D')]dL\\
&+ RR'LS_{21}(m_{12} - X')(m_{21} - X)dL'\\
&- T'S_{21}[R + M(m_{11} - D)][R' + M'(m_{22} - D')]dT\\
&+ (R(m_{21} - X)[R' + (m_{22} - D')(M' - L)]\\
&- TS_{21}[R + M(m_{11} - D)][R' + M'(m_{22} - D')])dT'\}/P \qquad (5)
\end{aligned}$$

$$P = TT'[R' + M'(m_{22} - D')][R + M(m_{11} - D)] \\ - RR'LL'(m_{12} - X')(m_{21} - X) \qquad (6)$$

dS_{22} and dS_{12} resulted from (4), (5) with the mentioned substitutions. X, X' errors stand for crosstalk measurements. D, M, R (D', M', R') errors are uniquely determined in terms of 3 standard loads A, B, C (A', B', C') and their 3 measurements a, b, c (a', b', c'), by full one–port VNA measurements, so the number of independent complex variables increases from 16 to 22. L, T (L', T') errors are accurately determined after the replacement of DUT with a direct thru (or approximately, if an adapter is used instead) in terms of new measurements t_{11}, t_{21} (t_{22}, t_{12}) and of previously found quantities. Their expressions were appropriately stated as

$$L = [\sum (ab + ct_{11})C(B - A)]/E \qquad (7)$$

$$T = (t_{21} - X)[\prod (A - B)(a - b)]/ \\ (E [\sum cC(B - A)]) \qquad (8)$$

$$E = \sum (ab + ct_{11})(B - A) \qquad (9)$$

where $\sum$ and $\prod$ produce two more terms, from the given one, by cyclic rotation of the letters a, b, c (a', b', c') or A, B, C (A', B', C'). In this way, each S–parameter has as total differential error dS, a sum of 22 differential terms:

16 due to measurement inaccuracies dm_{ij}, dX, dX', dt_{ij}, da, db, dc, da', db', dc' and 6 due to standard uncertainties given by their manufacturer dA, dB, dC, dA', dB', dC'. The expressions for dD, dM, dR (dD', dM', dR') are known [4]. The expressions for the rest of differential errors were developed as

$$dL = \{\sum (B - C)(b - t_{11})(c - t_{11})[(B - C)(b - a)(c - a)dA \\ - (b - c)(B - A)(C - A)da] + [\prod (A - B)(a - b)]\, dt_{11}\}/E^2 \qquad (10)$$

$$dT = \{\sum (t_{21} - X)(b - c)(B - C)[(t_{11} - c)(b - a)^2B(A^2 + C^2) \\ + (b - t_{11})(c - a)^2C(A^2 + B^2) - 2ABC(b - c)(t_{11}(b + c - 2a) \\ - bc + a^2)][(B - C)(b - a)(c - a)dA \\ - (b - c)(B - A)(C - A)da]\}/(E^2 [\sum cC(B - A)]^2) \\ + [\prod (A - B)(a - b)]\{[(t_{21} - X) \sum a(B - C)/E]dt_{11} \\ + dt_{21} - dX\}/(E [\sum cC(B - A)]) \qquad (11)$$

Each complex differential error defines a Differential Error Region (DER) on the complex plane with projections to coordinate axes the Differential Error Intervals (DEIs) [4]. Obviously, any quantity differentiably dependent on the above variables has also a DER. For example, after another correction to the given S to Z–parameters relations [5], the Z–DERs are resulted from

$$dZ_{11} = 2Z_0[(1 - S_{22})^2dS_{11} + (1 - S_{22})S_{21}dS_{12} + (1 - S_{22})S_{12}dS_{21} \\ + S_{12}S_{21}dS_{22}]/[(1 - S_{11})(1 - S_{22}) - S_{12}S_{21}]^2 \qquad (12)$$

$$dZ_{21} = 2Z_0[(1 - S_{22})S_{21}dS_{11} + S_{21}{}^2dS_{12} + (1 - S_{11})(1 - S_{22})dS_{21} \\ + (1 - S_{11})S_{21}dS_{22}]/[(1 - S_{11})(1 - S_{22}) - S_{12}S_{21}]^2 \qquad (13)$$

while dZ_{22}, dZ_{12} result from (12), (13) by application of the mentioned substitutions.

Results

Six calibration standards, in pairs of opposite sex, were used and their manufacturers' data were substituted in the developed expressions:

$A = -1 = A'$, $0 \le d|A| = d|A'| \le 0.01$, $-180° \le d\varphi_A = d\varphi_{A'} \le -178°$ or $178° \le d\varphi_A = d\varphi_{A'} \le 180°$,

$B = 0 = B'$, $|dB| = 0.029 = |dB'|$,

$C = 1 = C'$, $-0.01 \le d|C| = d|C'| \le 0$ and $-2° \le d\varphi_C = d\varphi_{C'} \le +2°$.

The inaccuracy of any VNA measurement was conservatively considered as a symmetric interval defined by just 1 unit in the last place of the corresponding mantissa, both in modulus and argument. Consequently, each S–DER is a sum of 20 parallelograms and 2 circles, with a contour of 160 vertices at most [4].

To demonstrate the method, a typical T–network of common resistors with nominal DC values Z_1 = 24.2 Ω, Z_2 = 120 Ω for the horizontal arms and Z_{12}=1.1 Ω for the vertical arm, were soldered on type–N base connectors of opposite sex and enclosed in an aluminium box, to form a two–port DUT.

The VNA measurement system was extended by two transmission lines of 3.66 m and 14 m, respectively, up to the DUT. The DUT was tested from 2 to 1289 MHz in 13 MHz steps. The frequency 1003 MHz was selected to illustrate the proposed method for S–DERs shown in Fig. 1.

To study the total differential error, dS was expressed as dU + dI, where dU is due to the uncertainty of 6 standards and dI to the inaccuracy of 16 measurements. The contribution of these, conservatively considered measurement inaccuracies to the total differential error is as much significant as the uncertainties of standard loads are. For example, computations for S_{12} over the whole measurement band show that max|dU| and max|dI| contribute ~35%–80% and ~25%–70% to max|dS_{12}|, respectively. In addition, Fig. 1 shows how the projections of each S–DER result its real and imaginary DEI. To display the variation of S–DER against frequency, a number of selected S–DER frames are shown in Fig. 2 as beads on a space–curved filament. It is worth mentioning that S_{11}–DER (S_{22}–DER) was greater than it resulted from appropriately organized full one–port measurements, as it was expected. Finally, the computed Z–DEIs are shown in Fig. 3, along with their LF Z-values.

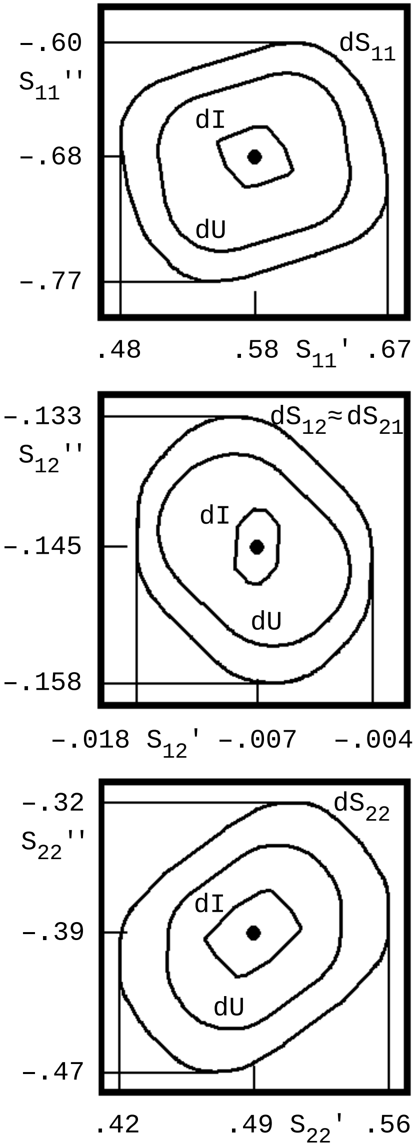

Fig.1: S–DERs at 1003 MHz

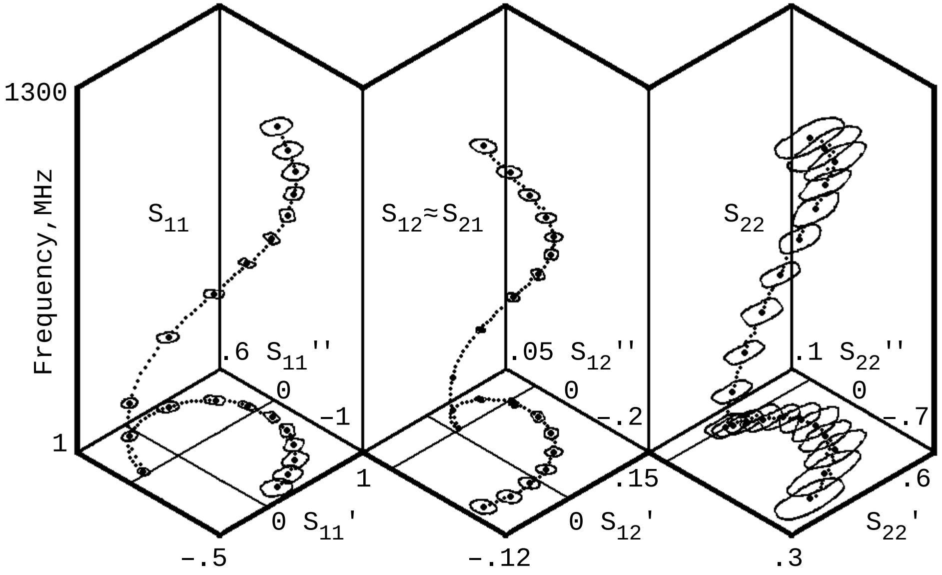

Fig.2: S–DERs against frequency

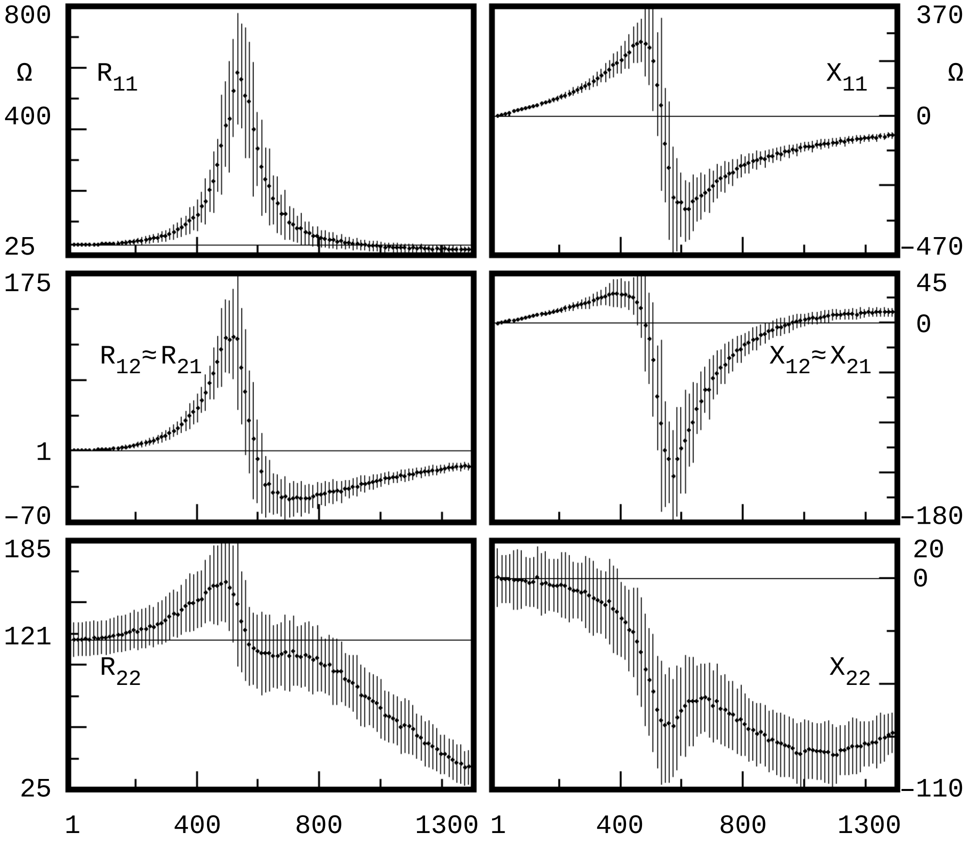

Fig.3: Z–DEIs against frequency

Conclusion

The proposed method may be efficiently used to estimate uncertainties in any case where the process equations (1), (2) and (4), (5) can find application.

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Total Differential Errors in One-Port Network Analyzer Measurements with Application to Antenna Impedance

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"http://arxiv.org/abs/physics/0703204"

Follow-Up Research Paper

S-Parameter Uncertainties in Network Analyzer Measurements with Application to Antenna Patterns

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FRONT COVER VIGNETTE

A faded synthesis of an anthemion rooted in a meandros

The thirteen-leaf is a symbol for a life tree leaf.
"Herakles and Kerberos", ca. 530–500 BC,
by Paseas, the Kerberos Painter,
Museum of Fine Arts, Boston.

www.mfa.org/collections/object/plate-153852

The simple meandros is a symbol for eternal immortality.
"Warrior with a phiale", ca. 480–460 BC,
by Berliner Maler,
Museo Archeologico Regionale "Antonio Salinas" di Palermo.

commons.wikimedia.org/wiki/File:Warrior_MAR_Palermo_NI2134.jpg